Daffodil International University

Microwave Engineering

ETE 415

LECTURE 5

IMPEDANCE MATCHING

Impedance Matching

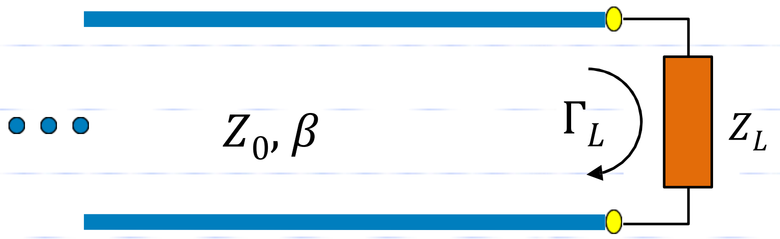
- Impedance matching (or simply "**matching**") one portion of a circuit to another is an immensely important part of MW engineering.
- Additional circuitry between the two parts of the original circuit may be needed to achieve this matching.

Why is impedance matching so important?

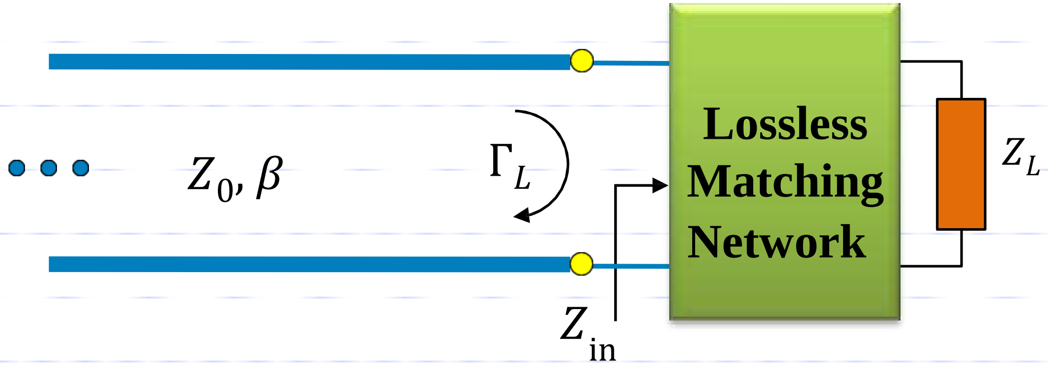
- **Maximum power** is delivered to a load when the TL is matched at both the load and source ends.
- With a properly matched TL, more signal power is transferred to the load, which increases the **sensitivity** of the device and improve the signal-to-noise ratio of the system.
- Some equipment (such as certain amplifiers) can be **damaged** when too much power is reflected back to the source.
- **Minimize** reflections.

Impedance Matching

- Consider the case of an arbitrary load that terminates a TL:



- To match the load to the TL, we require $\Gamma_L = 0$.
- However, if $Z_L \neq Z_0$ **additional circuitry** must be placed between Z_L and Z_0 to bring the VSWR = 1, or least approximately so:



For $\Gamma_L = 0$, this implies $Z_{\text{in}} = Z_0$. In other words, $R_{\text{in}} = \Re e[Z_0]$ and $X_{\text{in}} = 0$, if the TL is lossless.

Impedance Matching

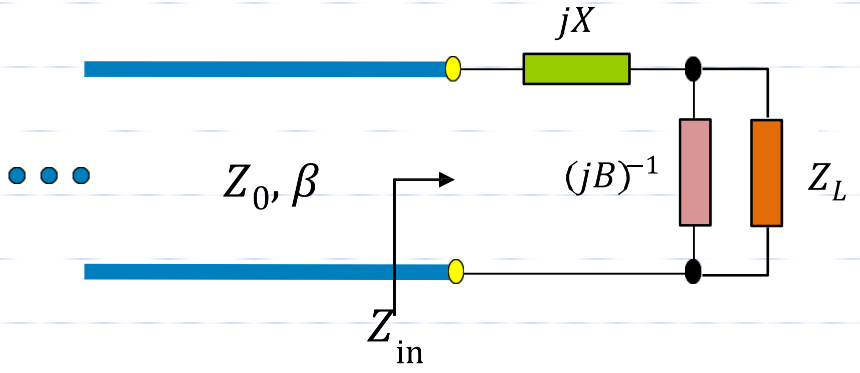
- We will discuss **three methods** for impedance matching in this course:
  - Matching with **L-Sections** (lumped elements)
  - **Stub** tuners (T-line)
  - **Quarter wave** impedance transformers.

- **Factors** that influence the choice of a matching network include:
  - Physical complexity
  - Bandwidth
  - Adjustability (to match a variable load impedance) Implementation

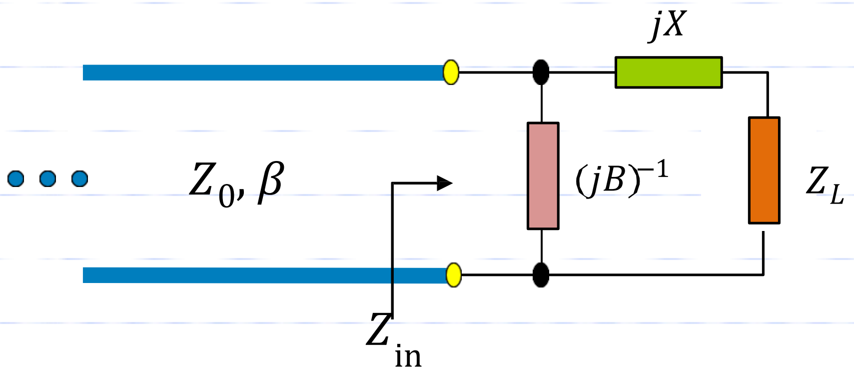
Matching with L-Sections

- Since it uses lumped elements, it is applicable **only** if the frequency is low enough, or the circuit size is small enough
- This network topology gets its name from the fact that the series and shunt elements of the matching network form an **"L" shape**.
- Two possible L-Sections:

$R_L > Z_0$



$R_L < Z_0$



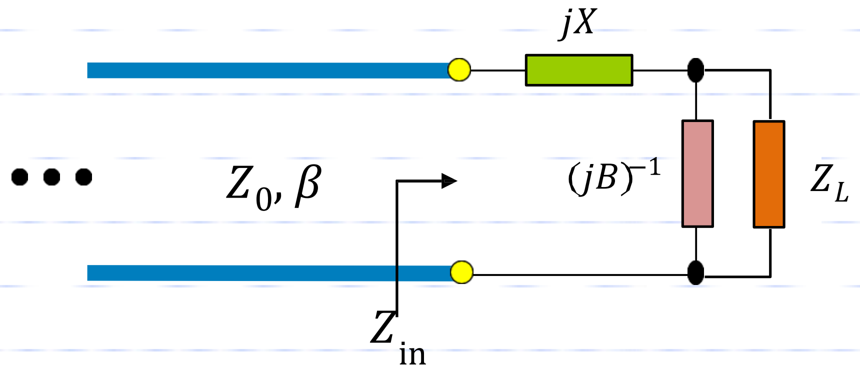
$$Z_{in} = Z_0 = jX + \left(jB + \frac{1}{R_L + jX_L}\right)^{-1} \qquad Z_{in} = Z_0 = \left(jB + \frac{1}{Z_L + jX}\right)^{-1}$$

➨ where $Z_L = R_L + jX_L$.

Example

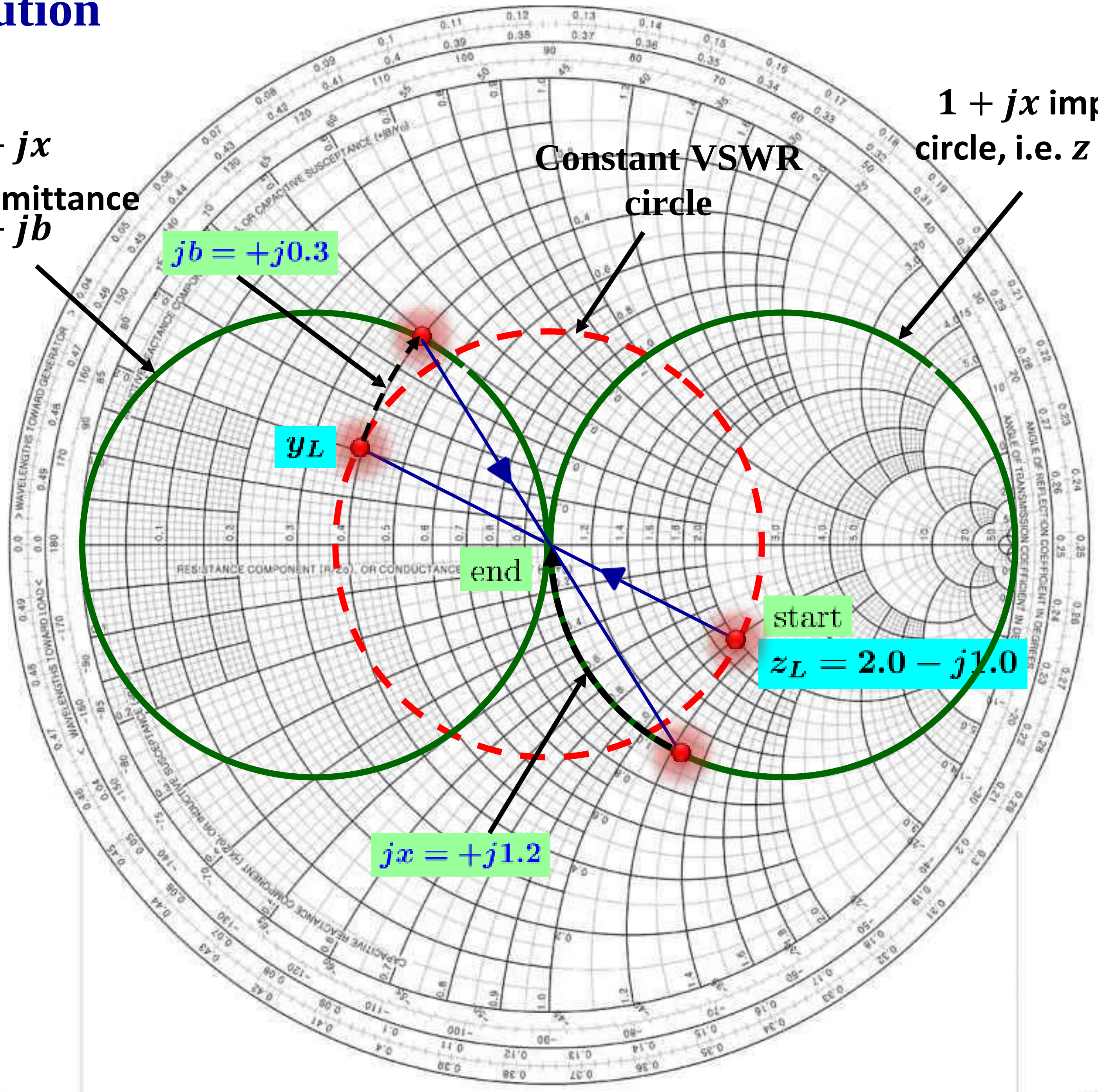
Design an L-section matching network to match a series RC load with an impedance $Z_L = 200 - j100\ \Omega$ to a 100 Ω line at a frequency of 500 MHz.

Since $R_L > Z_0$, we'll use the following circuit topology:



Normalization: $z_L = \frac{Z_L}{Z_0} = 2 - j1$ p.u.Ω

First solution



Solution

- Un-normalizing, we find that

$$jB = jb \cdot Y_0 = j0.3 \cdot \frac{1}{100} = j0.003 \text{ S}$$

$$jX = jx \cdot Z_0 = j1.2 \cdot 100 = j120\ \Omega$$

- What are the L and C values of these elements?

  - We can identify the type of element by the **sign of the reactance or susceptance**:

	Inductor	Capacitor
X	$Z_L = jwL$	$Z_C = \frac{1}{jwC} = \frac{-j}{wC}$
B	$Y_L = \frac{1}{jwL} = \frac{-j}{wL}$	$Y_C = jwC$

Solution

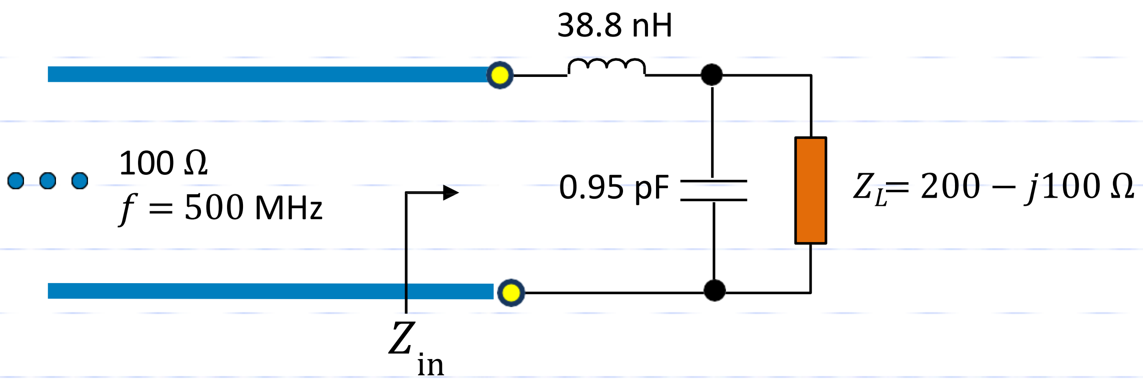
- Since $B > 0$, we identify this as a **capacitor**. Therefore,

$$jB = j\omega C = j0.003\ \text{S}$$

- For operation at 500 MHz, we need $C = \dfrac{0.003}{2\pi f} = 0.95\ \text{pF}$
- Since $X > 0$, we identify this as a **inductor**. Therefore,

$$jX = j\omega L = j120\ \Omega$$

- For operation at 500 MHz, we need $L = \dfrac{120}{2\pi f} = 38.8\ \text{nH}$
- The final circuit is:

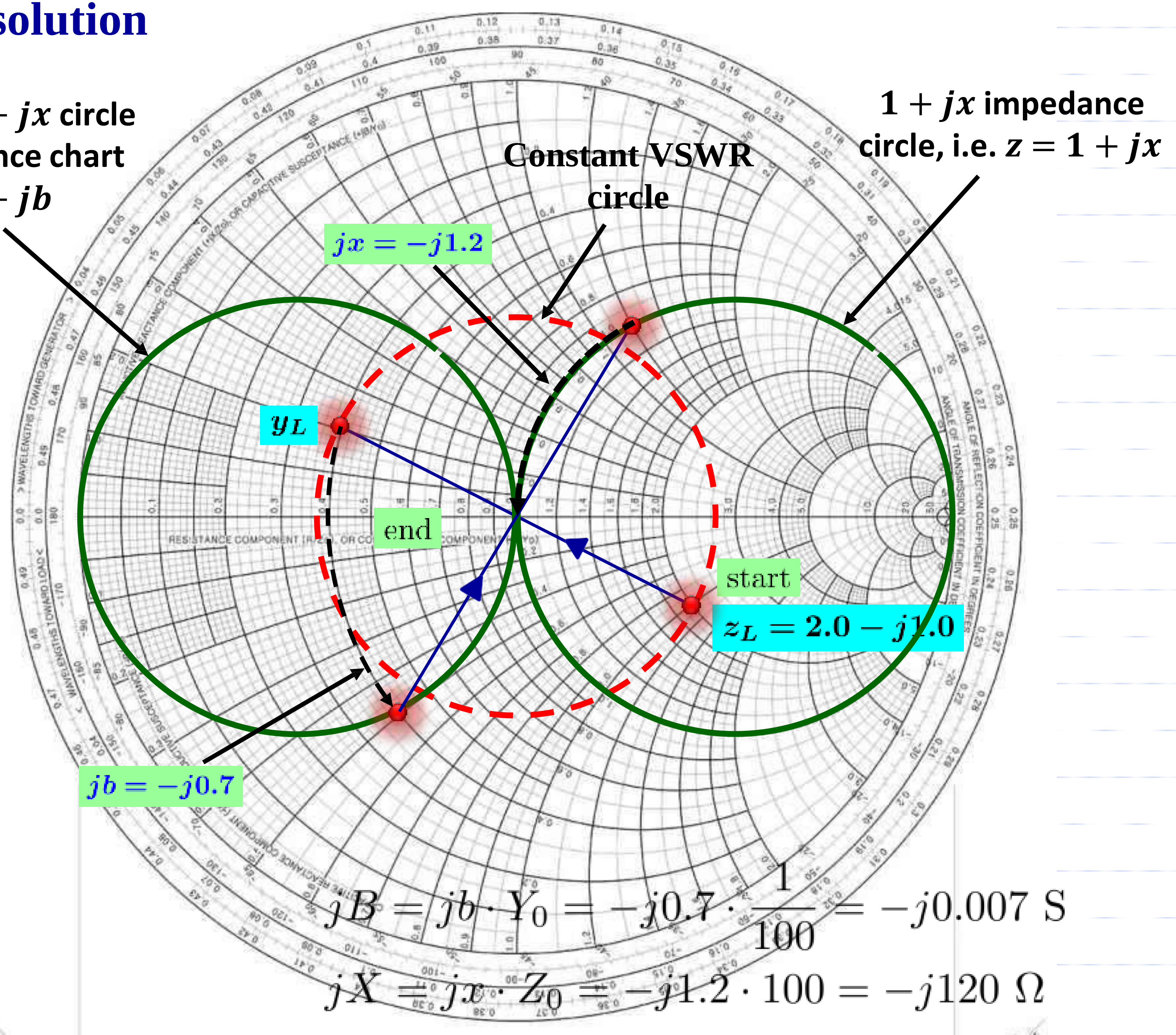


- Let's check to see if we have really achieved a match at 500 MHz:

$$Z_{\text{in}} = j2\pi f L + \left(j2\pi f C + \frac{1}{Z_L}\right)^{-1}$$

$$= j120 + 100 - j120 = 100 + j0\Omega$$

Second solution



$$jB = jb \cdot Y_0 = -j0.7 \cdot \frac{1}{100} = -j0.007 \text{ S}$$

$$jX = jx \cdot Z_0 = -j1.2 \cdot 100 = -j120\ \Omega$$

Solution

- Since $B < 0$, we identify this as a **inductor**. Therefore,

$$jB = \frac{-j}{wL} = -j0.007\ \text{S}$$

- For operation at 500 MHz, we need $L = \dfrac{1}{2\pi f B} = 45.47\ \text{nH}$

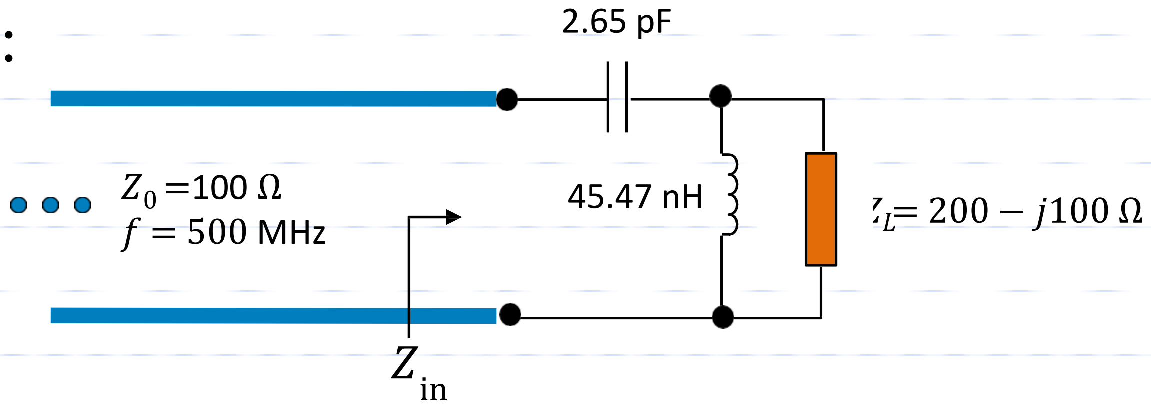
- Since $X < 0$, we identify this as a **capacitor**. Therefore,

$$jX = \frac{-j}{wC} = -j120\ \Omega$$

- For operation at 500 MHz, we need

$$C = \frac{1}{2\pi f X} = 2.65\ \text{pF}$$

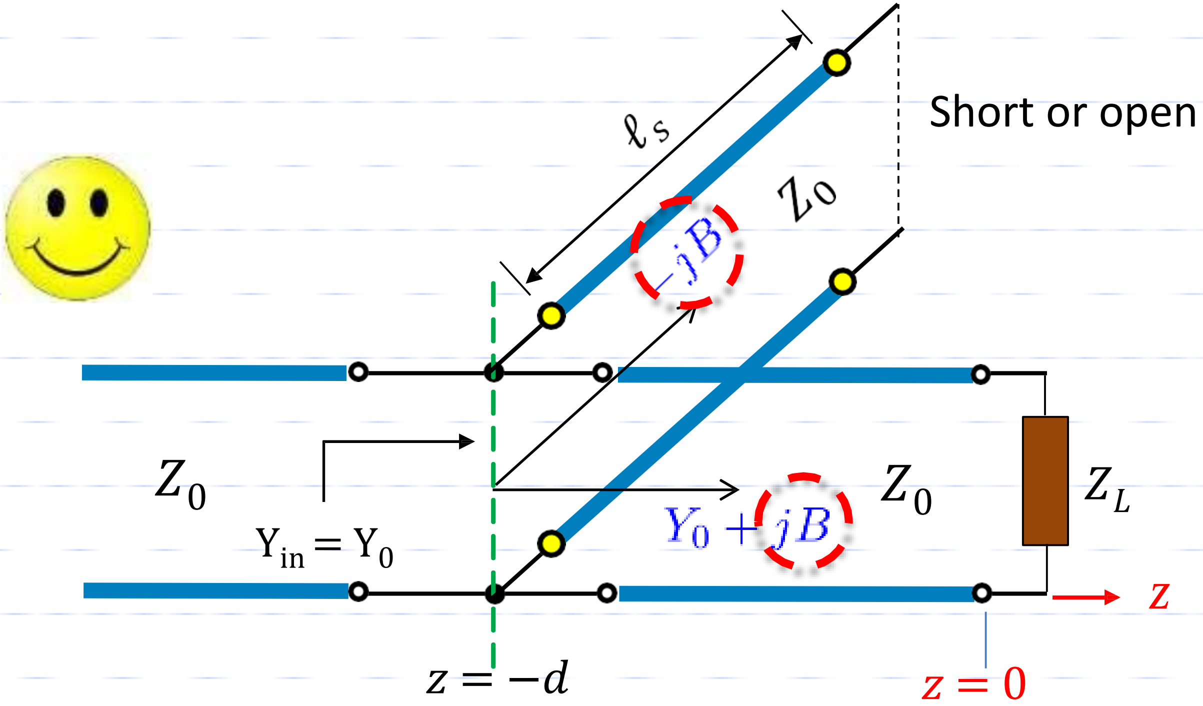
- The final circuit is:



Single-Stub Tuner (SST) Matching

- The SST uses a shorted or open section of TL attached at some position along another TL.
- It does not require lumped elements.
- It can be used for extremely high frequencies.
- It uses segments of T-lines with the **same Z_0** (**not necessary**) used for the feeding line.
- **Easy** to fabricate, the length can easily be made **adjustable** and little to **no power is dissipated** in the stub. (An open stub is sometimes easier to fabricate than a short.)
- It is very convenient for microstrip and stripline technologies.

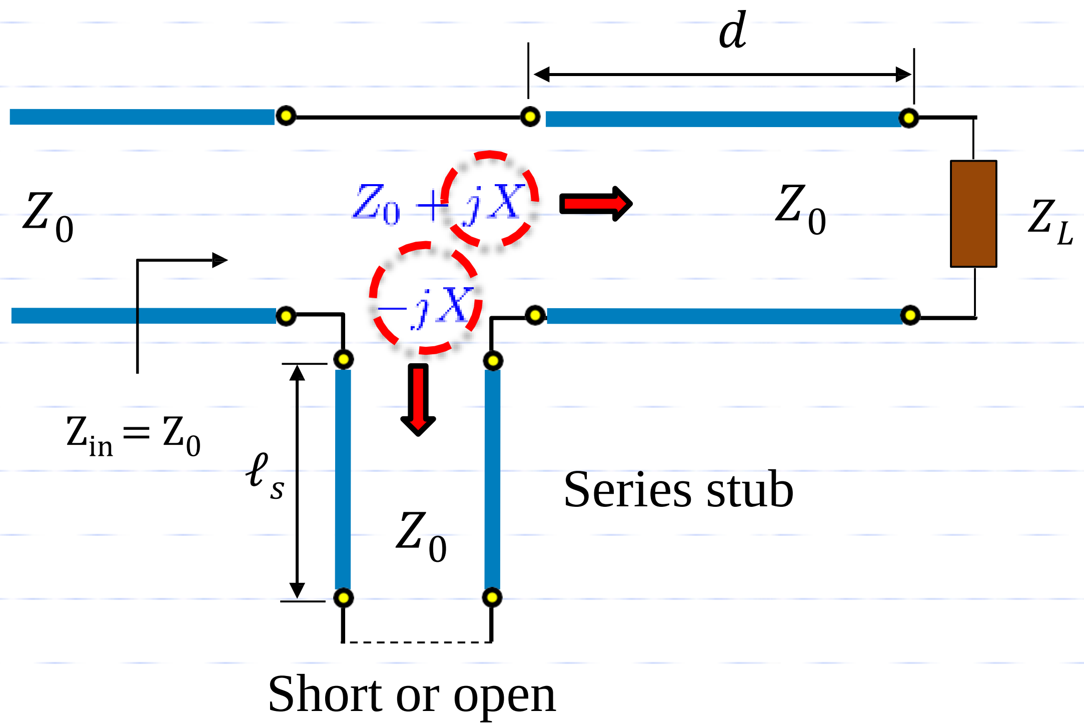
Single-Stub Shunt Matching



We only need to find d and ℓ_s

- First TL converts $Y_L = 1/Z_L$ to an admittance $Y_0 + jB$
- Second TL converts a short or an open to an admittance $-jB$

Single-Stub Series Matching

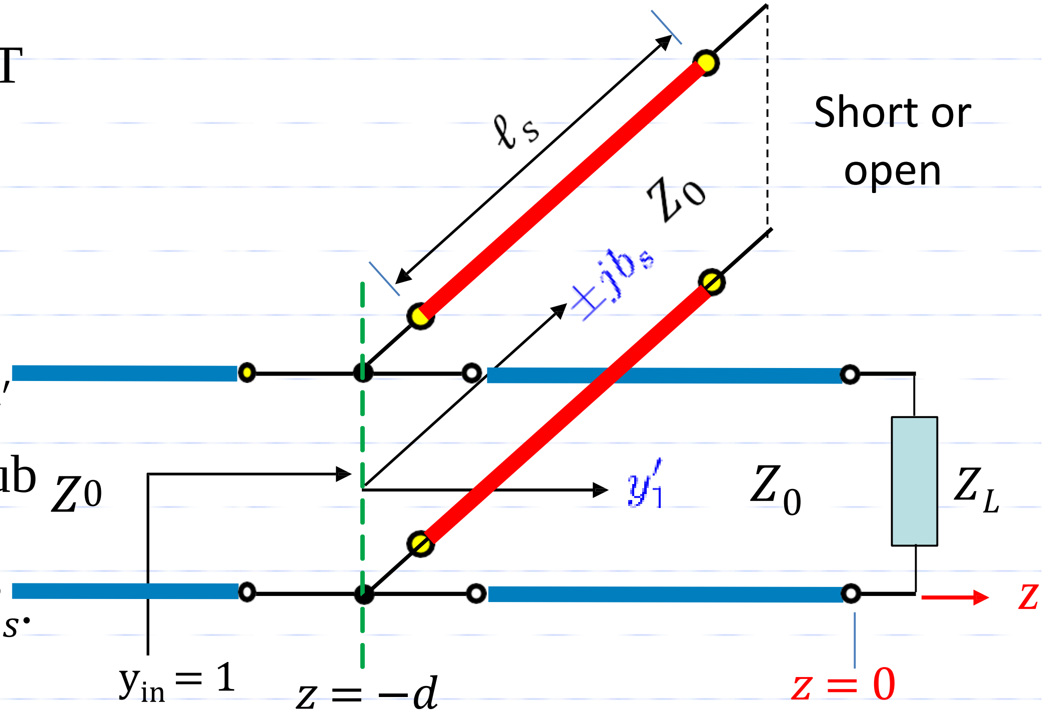


- **First** TL converts Z_L to an impedance $Z_0 + jX$
- **Second** TL converts a short or an open to an impedance $-jX$
- We only need to find d and ℓ_s

SST Using the Smith Chart

- In terms of quantities **normalized** to Z_0 or Y_0, the geometry is

- Recall that the operation of the SST requires that
  1. d is chosen such that y'_1 has a **real part = 1,** i.e., $y'_1 = 1 \pm jb_s$.
  2. The imaginary part of y'_1 is **negated** by the stub susceptance after choosing the proper length ℓ_s.

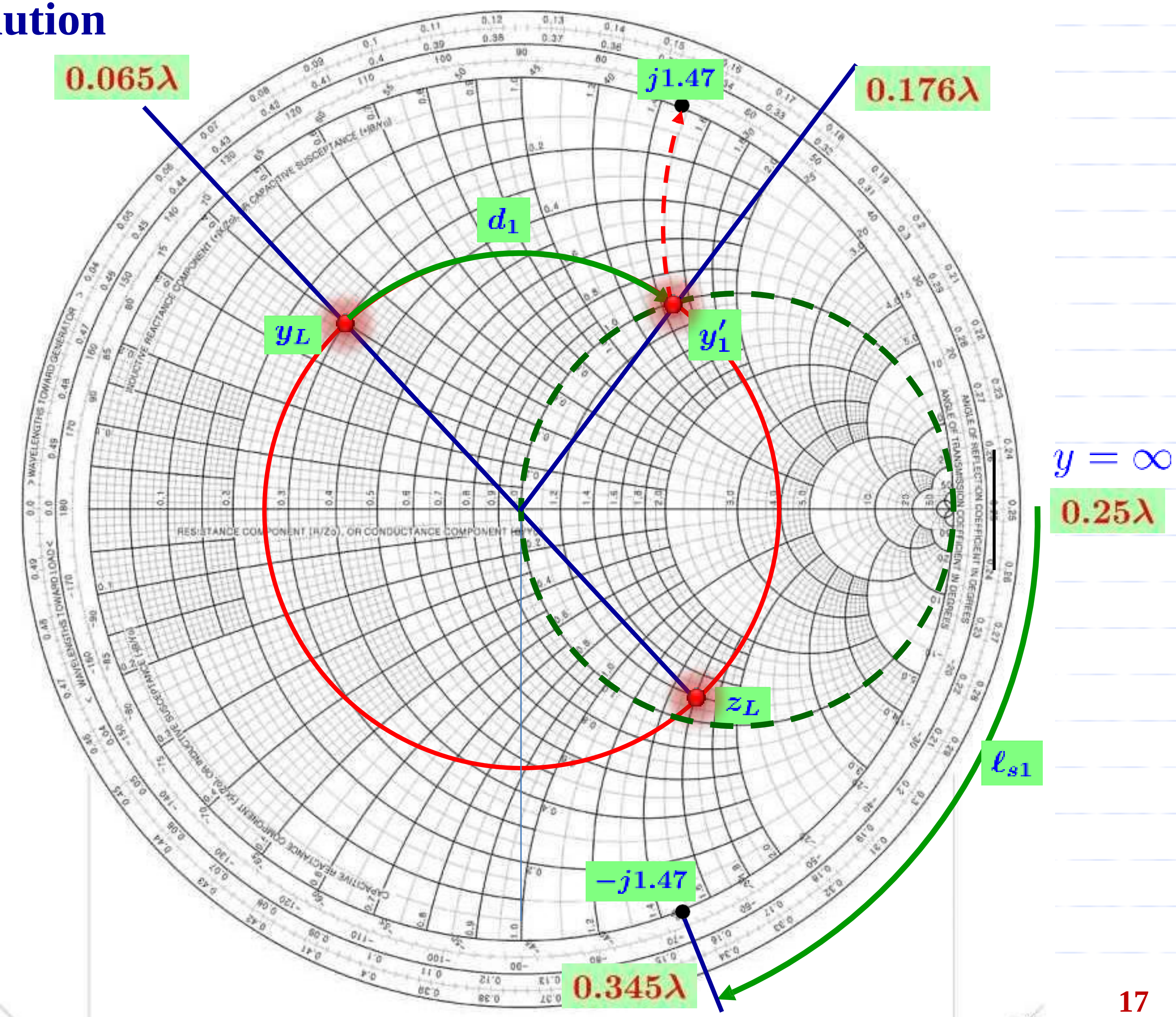


- This produces $y_{in} = 1$, which is the **matched state.**

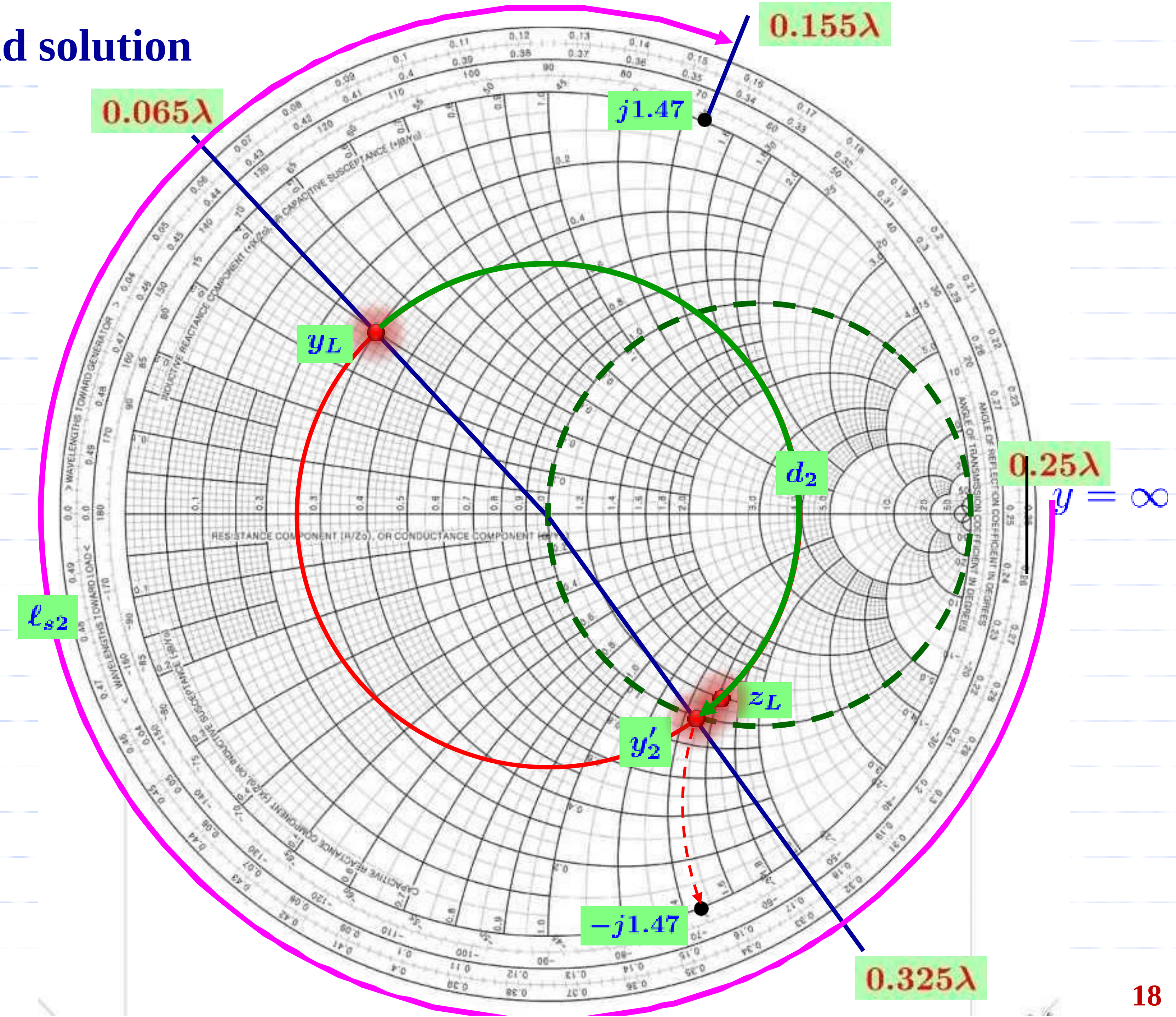
- **Example 5.2: Using the Smith chart, design a shorted shunt, single-stub tuner to match the load $Z_L = 60 - j80\ \Omega$ to a TL with characteristic impedance $Z_0 = 50\ \Omega$.**

- The normalized load impedance is: $z_L = 1.2 - j1.6$ p.u.Ω

First solution



Second solution



Solution: Smith

- There will be **two solutions**. Both of these give $y = 1 \pm jb_1$.
- For this example, we find from the Smith chart that

  (I) $y_1' = 1 + j1.47$

  (II) $y_2' = 1 - j1.47$

- From these rotations we can compute d as

  (I) $d_1 = 0.176\lambda - 0.065\lambda = 0.110\lambda$

  (II) $d_2 = 0.325\lambda - 0.065\lambda = 0.260\lambda$

- Next, find the stub lengths ℓ_s:

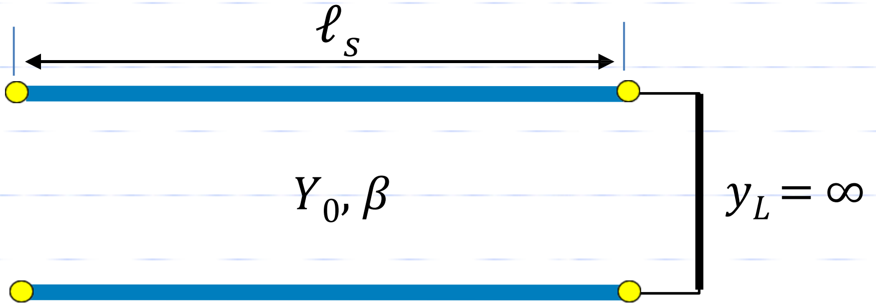
  (I) want $b_{s1} = -1.47$

  (II) want $b_{s2} = 1.47$

When either of these two susceptances is added to y_1', then $\boldsymbol{y_{in} = 1}$.

Solution: Smith

- The stub lengths can be determined directly from the Smith chart.



- On the Smith admittance chart, $\boldsymbol{y_L = \infty}$ **is located at** $\boldsymbol{\Re e\{\Gamma\} = 1}$**,** $\boldsymbol{\Im e\{\Gamma\} = 0}$. From there, rotate "wavelengths towards generator" to:

  (I) $b_s = -1.47 \quad \Rightarrow \quad \ell_{s1} = 0.345\lambda - 0.25\lambda = 0.095\lambda$

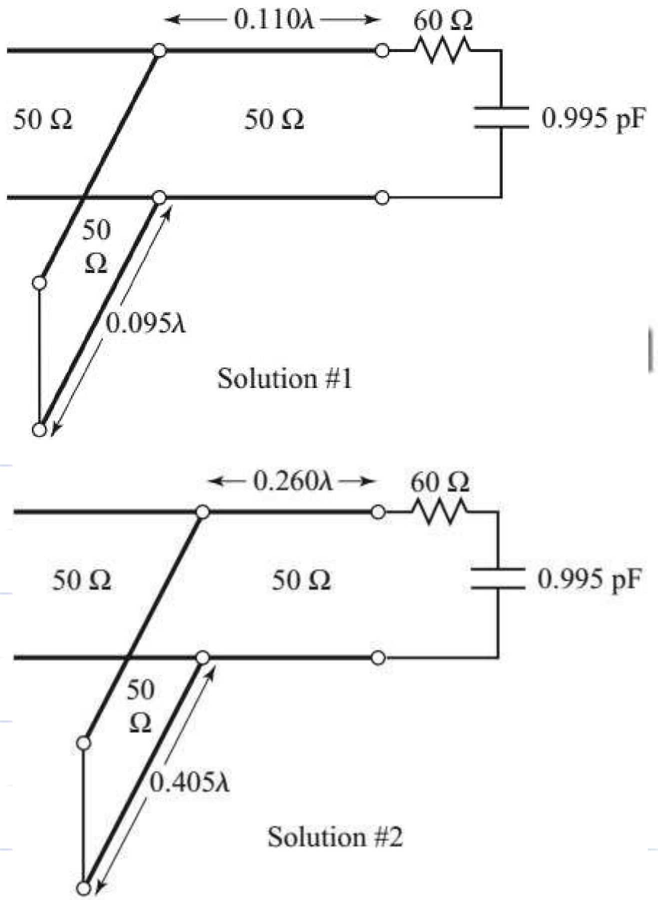
  (II) $b_s = +1.47 \quad \Rightarrow \quad \ell_{s2} = 0.25\lambda + 0.155\lambda = 0.405\lambda$

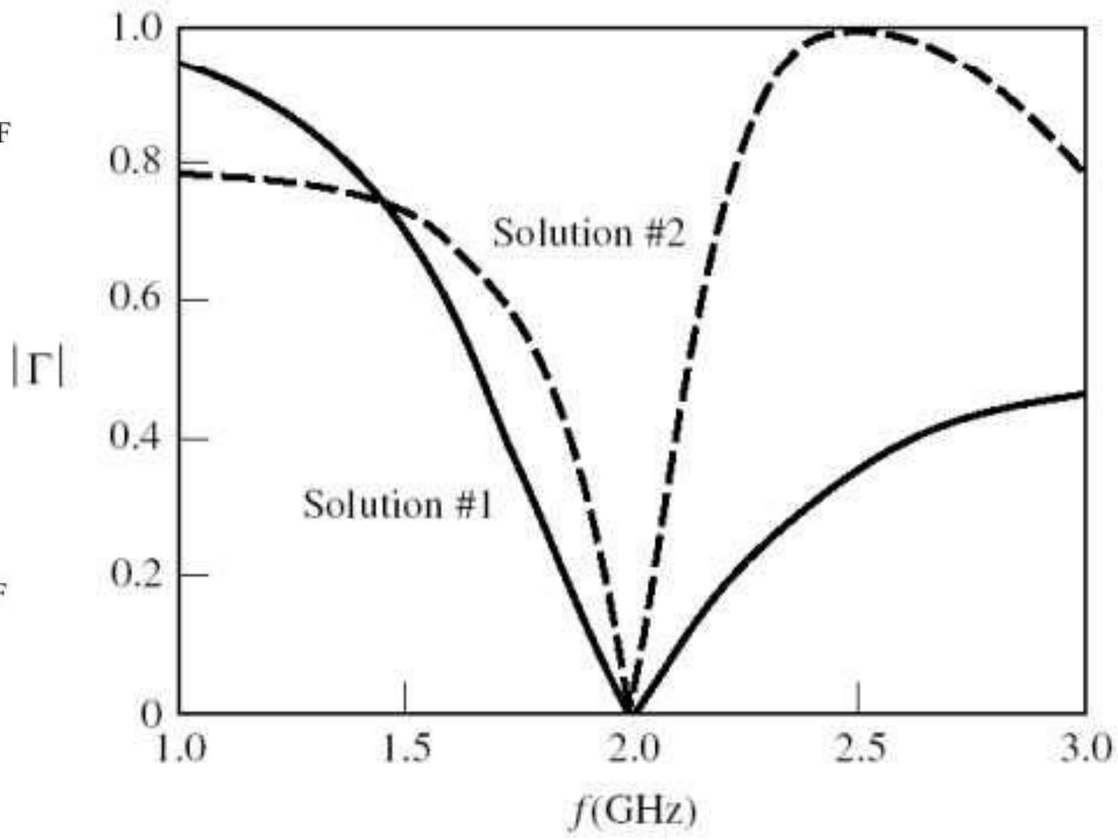
- The final two solutions are:

  (I) $d_1 = 0.110\lambda$ and $\ell_s = 0.095\lambda$

  (II) $d_2 = 0.260\lambda$ and $\ell_s = 0.405\lambda$

Solution: Smith



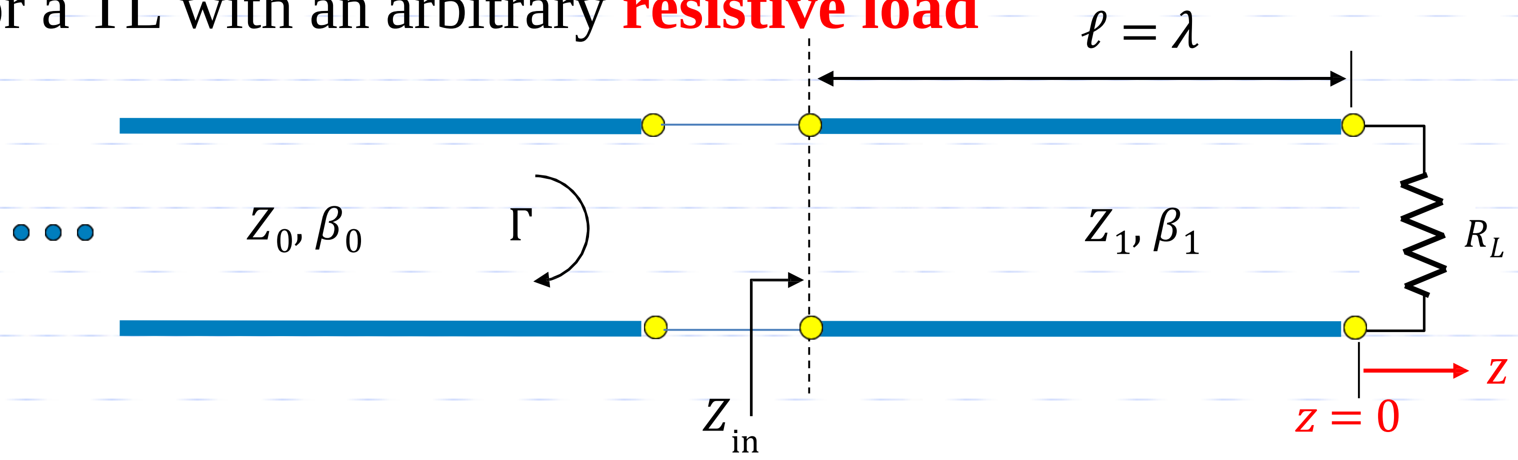


- **Solution 1** has a significantly better bandwidth than solution 2.
- Shorter stub produces wider bandwidth.

Quarter-Wave-Transformer Matching

- For a TL with an arbitrary **resistive load**

1 4



- the input impedance of the right-hand TL is given as

$$Z_{in} = Z_1 \frac{R_L + jZ_1 \tan(\beta_1 \ell)}{Z_1 + jR_L \tan(\beta_1 \ell)} \qquad (1)$$

- At $\ell = \lambda_1$ 4 $_1$ $\beta \ell = \frac{2\pi}{\lambda_1} \frac{\lambda_1}{} = \frac{\pi}{4}$ **electrical length**

$\Rightarrow$ 2 r

- Since $\tan \beta_1 l \to \infty$. Using this result in (1) gives

ad.

$$Z_{in} = \frac{Z_1^2}{R_L} \qquad (2)$$

Quarter-Wave-Transformer Matching

- This result is an interesting characteristic of TLs that are exactly $\lambda/4$ long.
- We can harness this characteristic to **design a matching network** using a $\lambda/4$ -length section of TL.

$$Z_1 = \sqrt{Z_0 R_L} \quad (3)$$

- Note that we can adjust Z_1 in (2) so that $\boldsymbol{Z_{in} = Z_0}$. In particular, from (2) with $Z_{in} = Z_0$ we find
- In other words, a $\lambda/4$ section of TL with this particular characteristic impedance will present a perfect match ($\Gamma = 0$) to the feedline (the left-hand TL).

This type of matching network is called a **quarter-wave transformer (QWT)**.

Disadvantages of QWTs

1. A TL must be **placed** between the load and the feedline.

1. A very **special characteristic impedance** (i.e., Z_1) for the QWT is required, which depends both on the load resistance, R_L, and the characteristic impedance of the feedline, Z_0.

1. QWTs work perfectly only for **one load at one frequency**. (Actually, it produces some bandwidth of “acceptable” VSWR on the TL, as do all real-life matching networks.)

Thank you Very Much !!!